

Joint Transmit and Receive Multi-user MIMO Decomposition Approach for the Downlink of Multi-user MIMO Systems

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Abstract— In this paper, we propose a joint transmit and receive decomposition approach for the downlink of multi-user MIMO systems. This approach makes use of the assumption of part of the receiver structure in computing the solution for the transmit processing. With this assumption, this approach decomposes a multi-user MIMO downlink channel into multiple parallel independent single-user MIMO downlink channels. A new degree of freedom is obtained by making the number of data streams variable. Sample simulation results are provided and these show the potential of the proposed scheme.

I. INTRODUCTION

Recently, the independence among user channels in a common medium has been recognized and been utilized to increase system capacity. The downlink multi-user MIMO decomposition was proposed independently in [1]-[4] for multi-user MIMO systems to increase system capacity. This decomposition of a multi-user MIMO system into several independent single-user MIMO systems is of significant practical importance, since any technique developed for single-user MIMO systems can be employed without modification in a multi-user environment. However, there are several drawbacks associated with this decomposition scheme. These include 1) the number of users is limited, 2) the number of receive antennas is limited, 3) the decomposition efficiency is low with respect to the transmit power in some situation, and 4) the solution does not exist in some cases.

Motivated by the restrictions of the multi-user MIMO decomposition, in this paper, we propose a joint transmit and receive multi-user MIMO decomposition scheme, which is an extension of the previous multi-user MIMO decomposition scheme proposed in [1]-[4]. This scheme offers considerable improvement in all aspects discussed above. The key properties of this proposed joint decomposition scheme include 1) the number of users can be as large as the number of transmit antennas, 2) the number of receive antennas is unlimited, 3) the decomposition efficiency is considerably improved, by allowing some interference to be removed by the receiver and therefore lifting the burden of the transmitter, and 4) the joint decomposition solution usually exists even in those cases that the previous multi-user MIMO decomposition solution does not. These improvements are made possible, by assuming some signal processing at the receiver, for the design of the transmit processing. The assumption of the special signal processing at the receiver is only used in order to find the solution of the transmit signal processing. It should be emphasized that our proposed joint multi-user MIMO decomposition scheme does not require the receiver to cooperate with the transmitter. The transmitter can carry out all computations itself. Finally, note that by making the number of data streams transmitted to each

user variable, new degrees of freedom are made available, which can be used to further optimise the system performance. Simulation results are provided and these show the outstanding potential of the proposed approach. In particular, it outperforms the previous decomposition approach significantly and is fairly close to the optimal approach.

II. SYSTEM MODEL AND BACKGROUND

We consider a multi-user MIMO system with M transmit antennas and K users as shown in Figure 1, where N_k antennas are located at the k -th user or mobile station (MS). At the base station (BS), the data are processed before transmission, which we refer to as transmit processing and which is our design target. Let \mathbf{b}_k represent the $L_k \times 1$ transmit data symbol vector for user k , where L_k is the number of parallel data streams transmitted simultaneously for user k ($k = 1, \dots, K$). This data symbol vector is passed through the transmit processing, which is characterized by the transmit matrix \mathbf{T}_k , a $M \times L_k$ matrix that takes in L_k nonzero values and outputs M terms. Each of the M output terms is transmitted by each of the M transmit antennas.

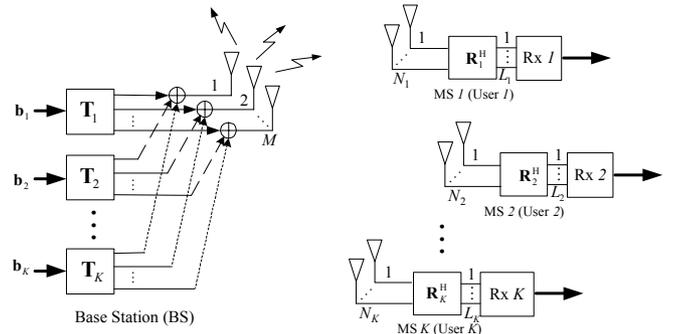


Figure 1. System configuration of a multi-MIMO system

We assume that the channel is flat fading and denote the MIMO channel to user k as \mathbf{H}_k , which is a $N_k \times M$ matrix. Its (i, j) -th element is the complex gain from the j -th transmit antenna at the BS to the i -th receive antenna at MS k . At the receiver of user k , N_k receive antennas are used to receive the L_k data symbols and the received signals can be written by a vector of length N_k , which is given by

$$\mathbf{y}_k = \mathbf{H}_k \sum_{i=1}^K \mathbf{T}_i \mathbf{b}_i + \mathbf{n}_k \quad (1)$$

where the noise \mathbf{n}_k is an $N_k \times 1$ vector, whose elements are i.i.d. zero mean complex Gaussian random variables with variance σ_n^2 . Without loss of generality, we assume the

elements of \mathbf{b}_k ($k=1,\dots,K$) are i.i.d. zero mean random variables and with unity variance. Also, it is assumed that the noise and data vectors are independent.

Based on the configuration mentioned above, our goal is to design a proper transmit processing for the downlink of a multi-user MIMO system to increase system capacity. One approach is to use the decomposition scheme independently proposed in [1]-[4]. However, it has a number of drawbacks as follows:

1. Number of users

Assuming all user channel-matrices \mathbf{H}_k ($k=1,2,\dots,K$), have full rank, the largest number K of users allowed must fulfill the inequalities $\sum_{i=1}^K N_i \leq M + N_k - 1$ for $k=1,2,\dots,K$. In the special case of $N_1=N_2=\dots=N_K=N$ the maximum number of users is upper bounded by

$$K \leq \frac{M+N-1}{N}. \quad (2)$$

For $N>1$, the number of users cannot exceed $(M+1)/2$, which is a serious limitation, that gets even worse with increasing number of receive antennas.

2. Number of receive antennas

The number of receive antennas is also limited. From (2), it follows, that $N \leq M - 1$, if we want to be able to serve at least two users.

3. Transmission efficiency

Depending on the channel, the realization of the MU-MIMO decomposition by transmit signal processing may become inefficient with respect to transmit power. If the null-space $\text{null}(\mathbf{H}_k)$ has large overlap with the joint null-space $\bigcap_{i=1, i \neq k}^K \text{null}(\mathbf{H}_i)$, excessive transmit power is needed to achieve the decomposition.

4. Existence of solution

In the case $\text{null}(\mathbf{H}_k) \equiv \bigcap_{i=1, i \neq k}^K \text{null}(\mathbf{H}_i)$, the decomposition does not exist at all. This happens for instance in a spatially semi-correlated channel [5], where the directions of departure waves are identical for all users.

In this paper, we wish to devise a method that overcomes these limitations. The inspiration for our idea comes about by noting that this decomposition scheme does not use any assumption at the receivers and that the transmit processing is obtained by only considering the multi-user channel. The last two drawbacks discussed above are a consequence of the properties of the multi-user channel. It can be expected, that good improvement will be possible, if a way can be found to change the properties of the multi-user channel in order to make it more friendly for decomposition. In following, we assume that each user employs a *pre-receiver* (front part of the receiver) to filter the signal according to the channel and the transmit processing. By denoting the pre-receiver weight for user k as \mathbf{R}_k , which is a $N_k \times L_k$ matrix, the output signal after passing through the pre-receiver can be written as a vector of length L_k , which is given by $\hat{\mathbf{y}}_k = \mathbf{R}_k^H \mathbf{y}_k$.

III. JOINT TRANSMIT AND RECEIVE MULTI-USER MIMO DECOMPOSITION

A. Transmitter and Receiver Structure

We solve the problem in two steps. In the first step, we assume the *pre-receiver* filter matrices \mathbf{R}_k are known. By considering the pre-receiver being part of the channel, we can write the transmit weight \mathbf{T}_k according to the decomposition solution [2] as $\mathbf{T}_k = \mathbf{V}_k \mathbf{A}_k$, where \mathbf{V}_k is chosen such that $\mathbf{R}_i^H \mathbf{H}_i \mathbf{V}_k = \mathbf{0}$ for $i \neq k$ and \mathbf{V}_k has orthogonal columns. We can compute \mathbf{V}_k by singular value decomposition

$$\begin{bmatrix} \mathbf{R}_1^H \mathbf{H}_1 \\ \vdots \\ \mathbf{R}_{k-1}^H \mathbf{H}_{k-1} \\ \mathbf{R}_{k+1}^H \mathbf{H}_{k+1} \\ \vdots \\ \mathbf{R}_K^H \mathbf{H}_K \end{bmatrix} = [\tilde{\mathbf{U}}_k \quad \mathbf{U}_k] \cdot \begin{bmatrix} \Sigma & \mathbf{0} \\ \mathbf{0} & \mathbf{0} \end{bmatrix} \cdot \begin{bmatrix} \tilde{\mathbf{V}}_k^H \\ \mathbf{V}_k^H \end{bmatrix}. \quad (3)$$

Therefore, we can obtain

$$\hat{\mathbf{y}}_k = \mathbf{R}_k^H \mathbf{H}_k \mathbf{T}_k \mathbf{b}_k + \mathbf{R}_k^H \mathbf{n}_k = \mathbf{R}_k^H \mathbf{H}_k \mathbf{V}_k \mathbf{A}_k \mathbf{b}_k + \mathbf{R}_k^H \mathbf{n}_k. \quad (4)$$

Note that the multi-user MIMO system has been decoupled interference-free into K parallel single-user MIMO systems. Also, note that in general $\mathbf{H}_i \mathbf{V}_k \neq \mathbf{0}$, for $i \neq k$, which means that some amount of multi-user interference is present at the input of the receivers. A close observation of (4) shows that we can think of the equivalent single-user MIMO channel of user k as $\mathbf{H}_k \mathbf{V}_k$ with the transmit and pre-receive processing represented by \mathbf{A}_k and \mathbf{R}_k , respectively.

In the second step, assume that all the transmit weights \mathbf{T}_k ($k=1,\dots,K$) are set up at the transmitter according to the decomposition structure described above, the output of the pre-receivers given in (4) can be written as

$$\hat{\mathbf{y}}_k = \mathbf{R}_k^H \mathbf{F}_k \mathbf{A}_k \mathbf{b}_k + \mathbf{R}_k^H \mathbf{n}_k. \quad (5)$$

where $\mathbf{F}_k = \mathbf{H}_k \mathbf{V}_k$ is the effective channel from the receiver's point of view. Let us write the matrix \mathbf{A}_k in the form $\mathbf{A}_k = \mathbf{Q}_k \mathbf{P}_k^{1/2}$, where \mathbf{Q}_k has orthonormal columns and \mathbf{P}_k is non-negative definite diagonal matrix containing the values for transmit power for each data stream of user k , and $P_k = \text{trace}(\mathbf{P}_k)$ is the transmit power assigned to user k . The overall transmit power then is given by $P_T = \sum_{k=1}^K P_k$.

Without loss of mutual information, the channel can be decomposed into independent sub-channels by singular value decomposition of \mathbf{F}_k .

$$\mathbf{F}_k = \mathbf{H}_k \mathbf{V}_k = [\mathbf{R}_k \quad \mathbf{U}'] \cdot \begin{bmatrix} \Sigma_k & \mathbf{0} \\ \mathbf{0} & \Sigma' \end{bmatrix} \cdot \begin{bmatrix} \mathbf{Q}_k^H \\ \mathbf{V}_k^H \end{bmatrix}. \quad (6)$$

Since there are only L_k independent data streams to be transmitted to user k , the receive weight \mathbf{R}_k is chosen as the L_k left singular vectors corresponding to the L_k largest singular values of \mathbf{F}_k . At the same time, \mathbf{Q}_k is chosen as the L_k right-singular vectors corresponding to the L_k largest

singular values, i.e., $\hat{\mathbf{y}}_k = \mathbf{\Sigma}_k \mathbf{P}_k^{1/2} \mathbf{b}_k + \mathbf{n}'_k$, where $\mathbf{\Sigma}_k$ is a $L_k \times L_k$ diagonal matrix, containing the L_k dominant singular values of \mathbf{F}_k , and \mathbf{n}'_k is a L_k dimensional noise vector, whose elements are i.i.d. zero-mean complex Gaussian entries with variance σ_n^2 , since $\mathbf{R}_k^H \mathbf{R}_k = \mathbf{I}$. Hence, the noise is unchanged in power and spatially white. The diagonal entries of the transmit power matrix \mathbf{P}_k can now be chosen, according to the ‘waterfilling’ policy [6], based on the singular values from $\mathbf{\Sigma}_k$ and the total power P_k assigned to this user. Since the column vectors of \mathbf{R}_k span the subspace of the arriving dedicated signals $\mathbf{H}_k \mathbf{V}_k \mathbf{A}_k \mathbf{b}_k = \mathbf{R}_k \mathbf{\Sigma}_k \mathbf{P}_k^{1/2} \mathbf{b}_k$, the receive matrix captures the complete dedicated signal for user k . Together with the property of unchanged noise, this means that the matrix \mathbf{R}_k does not change mutual information. Therefore, the channel capacity is the same, regardless if the matrix \mathbf{R}_k is present or not.

For sake of simplicity, we assume that all the users have the same number of receive antennas and the same number of data streams. That is, $N_1 = \dots = N_K = N$ and $L_1 = \dots = L_K = L$. The dimension of the null-space spanned by the column vectors of \mathbf{V}_k is then given by $d = \text{rank}(\mathbf{V}_k) = M - L \cdot (K - 1)$.

In order to be able to transmit L data streams, we need to have $d \geq L$. Furthermore since $1 \leq L \leq N$, the number of data streams can be given by

$$1 \leq L \leq \min\{N, M/K\}, \quad (7)$$

and the number of users $K \leq M$, which is independent of the number of receive antennas.

B. Joint Decomposition Algorithm

Since the transmit weight \mathbf{V}_k ($k = 1, \dots, K$) is a function of the pre-receiver weight \mathbf{R}_k ($k = 1, \dots, K$) and the pre-receiver weight \mathbf{R}_k ($k = 1, \dots, K$) on the other hand is a function of the transmit weight \mathbf{V}_k ($k = 1, \dots, K$), we propose an iterative algorithm which computes both matrices jointly. Given a particular value of the number of data streams, L_k ($k = 1, \dots, K$), the iterative procedure can be given as follows.

Procedure for Computing Joint Decomposition

Inputs:

- All channel matrices \mathbf{H}_k ($k = 1, 2, \dots, K$).
- The number of data streams L_k ($k = 1, 2, \dots, K$).
- The transmit powers P_k ($k = 1, 2, \dots, K$).

Outputs:

- The transmit matrices \mathbf{T}_k ($k = 1, 2, \dots, K$).

Step 1: Calculate an initial virtual receiver weight $\mathbf{R}_k^{(i=0)}$ ($k = 1, \dots, K$) by applying (6) and assuming the transmit weight matrix \mathbf{V}_k ($k = 1, \dots, K$) is identity.

Step 2: Calculate the transmit weight $\mathbf{V}_k^{(i=0)}$ ($k = 1, \dots, K$) by using (3) and $\mathbf{R}_k^{(i=0)}$ ($k = 1, \dots, K$).

Step 3: Compute the virtual receiver weight $\mathbf{R}_k^{(i+1)}$ ($k = 1, \dots, K$) as the L_k dominant left-singular vectors of the matrix $\mathbf{H}_k \mathbf{V}_k^{(i)}$ ($k = 1, \dots, K$) by applying (6).

Step 4: Compute the transmit weight $\mathbf{V}_k^{(i+1)}$ ($k = 1, \dots, K$) by using (3) and $\mathbf{R}_k^{(i+1)}$ ($k = 1, \dots, K$).

Step 5: Repeat Step 3 and Step 4 until the projector of the virtual receiver weight matrix converges. That is, $\|\mathbf{P}_{\mathbf{R}_k}^{(i+1)} - \mathbf{P}_{\mathbf{R}_k}^{(i)}\|_F^2 / \|\mathbf{P}_{\mathbf{R}_k}^{(i+1)}\|_F^2 < \varepsilon_1$ for all k where $\mathbf{P}_{\mathbf{R}_k}^{(i)} = \mathbf{R}_k^{(i)} \mathbf{R}_k^{(i)H}$ and $\|\cdot\|_F^2$ is the squared Frobenius norm. In our simulation, we use $\varepsilon_1 = 0.01\%$

Step 6: Compute \mathbf{Q}_k ($k = 1, \dots, K$) as the L_k ($k = 1, \dots, K$) dominant right singular vectors of $\mathbf{H}_k \mathbf{V}_k^{(i+1)}$ ($k = 1, \dots, K$).

Step 7: Compute the stream power distribution matrix \mathbf{P}_k ($k = 1, \dots, K$). If mutual information is to be maximized this has to be done according to the ‘waterfilling’ policy [6] based on the singular values of $\mathbf{H}_k \mathbf{V}_k^{(i+1)}$ ($k = 1, \dots, K$) and the power P_k ($k = 1, \dots, K$) assigned for the users.

Step 8: Finally, form the transmit weights $\mathbf{T}_k = \mathbf{V}_k^{(i+1)} \mathbf{Q}_k \mathbf{P}_k^{1/2}$ ($k = 1, \dots, K$).

This algorithm computes the equilibrium solution of the processing. There is no co-operation among the transmitter and the receivers. To be more specific, in Step 4 of the algorithm, the transmitter chooses its optimum transmit strategies after all receivers have decided upon their pre-receive weights. On the other hand, in Step 3 each receiver chooses its optimum receive weights after the transmitter has decided upon its transmit weights. The successive repetition of Steps 3 and 4 is looking for an equilibrium of this non-cooperative process. Note that Steps 1 and 2 provide initial values.

One peculiarity of this algorithm is that the pre-receive weight matrix \mathbf{R}_k can be replaced by $\mathbf{R}_k \mathbf{Q}$, with any invertible matrix \mathbf{Q} , without changing mutual information. Since any $\mathbf{R}_k \mathbf{Q}$ is equally suitable as the virtual receiver matrix, we use the projector onto the column space of \mathbf{R}_k in Step 5, as all $\mathbf{R}_k \mathbf{Q}$ have the same column space.

Note that the number of data streams L_k transmitted to each user offers additional degrees of freedom, which can be used to optimize the system performance further. In our simulations, we choose L_k such as to maximize the minimum mutual information among the users.

This scheme offers considerable improvement in all aspects discussed in Section II. This joint decomposition scheme has the following key characteristics:

1. The number of users K can be as large as the number of transmit antennas M . From (7), we can see that the number of users $K \leq M$, in which the equality holds when the number of data streams $L_k = L = 1$ ($k = 1, \dots, K$).
2. The number of receive antennas is unlimited. This can be seen from (7).

3. The transmission efficiency is considerably improved by allowing some interference to be removed by the receiver, and therefore lifting the burden of the transmitter. This can be justified from the performance improvement compared to the standard multi-user MIMO decomposition scheme.
4. The solution for the transmit processing usually exists even in the case $\text{null}(\mathbf{H}_k) \equiv \bigcap_{i=1, i \neq k}^K (\mathbf{H}_i)$, which makes the new scheme suitable for the spatial semi-correlated channel with same directions of departing waves for all users, as discussed in Section II. We justify this by providing numerical results in Section IV.

Also, note that by making the number of data streams transmitted to each user variable, new degrees of freedom are made available, which can be used to further optimize the system performance. It should be emphasized that the assumption of the pre-receiver structure is just a means to obtain the transmit processing. Each user can have its own receiver structure.

We are not able to show the convergence of this algorithm theoretically. Further research needs to be carried out for discussing the behavior of this algorithm. To this point, all our simulation results however show that it is convergent. Nevertheless, this verifies the practical potential of this algorithm. We refer to this scheme as *Joint Transmit and Receive Multi-user MIMO Decomposition Scheme*.

IV. SIMULATION RESULTS

The performance of the proposed scheme discussed above is investigated by computer simulation. In our simulation, we assume that the noise variance (σ_n^2) is one. The flat fading multi-user MIMO channel, including the uncorrelated and spatially correlated models [5], is used. Two different total transmit powers, $P_T/\sigma_n^2 = 5$ dB and 15 dB, are investigated. We choose the *capacity CDF* (*cumulative probability density function*) as our performance evaluation measure. Since the theoretical capacity of the downlink of a multi-user MIMO channel is still an open question, we define the capacity in our simulation as the minimum mutual information among the users, assuming single-user decoding. This is an important representative index to measure the capacity of the downlink in a multi-user system. Provided the noise and all transmitted signals are independent, the mutual information for a particular user, say user k , is given by

$$I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k) = H(\mathbf{y}_k | \mathbf{T}, \mathbf{H}_k) - H(\mathbf{y}_k | \mathbf{b}_k, \mathbf{T}, \mathbf{H}_k). \quad (8)$$

Note that we represent \mathbf{T}_k ($k = 1, \dots, K$) as \mathbf{T} . If the noise \mathbf{n}_k and all transmitted data \mathbf{b}_k are zero mean and i.i.d. Gaussian distributed with variance σ_n^2 and unity as well, from (8) we can obtain the mutual information of user k as

$$I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k) = \log_2 \det \left(\mathbf{I} + \mathbf{T}_k^H \mathbf{H}_k^H \left[\sigma_n^2 \mathbf{I} + \mathbf{H}_k \sum_{i=1, i \neq k}^K \mathbf{T}_i \mathbf{T}_i^H \mathbf{H}_i^H \right]^{-1} \mathbf{H}_k \mathbf{T}_k \right). \quad (9)$$

Hence, the capacity we define can be expressed as $C = \min_k \{I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k), k = 1, \dots, K\}$. Due to the

randomness of the channel matrix \mathbf{H}_k ($k = 1, \dots, K$), the capacity we define is a random variable, which can be described by its probability density function (pdf), $f_C(C)$, and therefore the *capacity CDF* is defined as $F_C(C) = \int_0^C f_C(x) dx$.

Based on this performance evaluation measure, the Joint Transmit and Receive MU-MIMO Decomposition Scheme (denoted by Joint MU-MIMO Decomposition) is compared with the standard MU-MIMO Decomposition Scheme proposed in [1]-[4] (denoted by MU-MIMO Decomposition), the optimal scheme (denoted by Optimal), and a time division scheme (denoted by TDMA). The optimal scheme is obtained by nonlinear optimization, which maximizes the minimum mutual information among the users. That is,

$$\mathbf{T} = \arg \max_{\mathbf{T}} \min \{I_k(\mathbf{T}), k = 1, \dots, K\} \text{ s.t. } \text{trace}(\mathbf{T}\mathbf{T}^H) = P_T \quad (10)$$

where $I_k(\mathbf{T}) = I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k)$ is a function of \mathbf{T} . This nonlinear optimization is solved numerically. A Sequential Quadratic Programming (SQP) method [7] is used. On the other hand, the time division scheme divides the multiple users in time and therefore, at any time instant there is only one user transmitting. For sake of comparison, the mutual information of user k in this scheme is given by

$$I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k) = \frac{1}{K} \log_2 \det \left(\mathbf{I} + \frac{1}{\sigma_n^2} \mathbf{T}_k^H \mathbf{H}_k^H \mathbf{H}_k \mathbf{T}_k \right), \quad (11)$$

where \mathbf{T}_k is chosen to maximize $I_k(\mathbf{b}_k; \mathbf{y}_k | \mathbf{T}, \mathbf{H}_k)$ subject to the total average transmit power (i.e., $\text{trace}(\mathbf{T}_k \mathbf{T}_k^H) = P_T$). The factor $1/K$ in (11) is because of the time division that each user only has $1/K$ of the time for transmission. The analytical solution for \mathbf{T}_k can be obtained in this scheme and it is chosen according to [8] to maximize the mutual information subject to the power constraint $\text{trace}(\mathbf{T}_k \mathbf{T}_k^H) = P_T$.

Throughout this section, we consider a K -user system with M transmit antennas at the BS and N receive antennas at each MS and we will refer to it as a $M \times (N_1, N_2, \dots, N_K)$ system. Also, we assume that the number of data streams is equal to L for each user. Finally, note that we select the number of data stream $L_1 = L_2 = \dots = L_K = L$ for the two proposed example schemes by maximizing the defined capacity C .

Figure 2 to Figure 4 present the capacity CDF for configurations $5 \times (3,3)$, $4 \times (2,2,2)$ and $6 \times (2,2)$ in an uncorrelated channel, respectively. It can be seen that the proposed scheme outperforms the time division scheme significantly. Also, we can see that it has better performance than the standard MU-MIMO decomposition scheme. As we expected, the proposed scheme is more flexible in that it works well in all configurations, including those for which the standard MU-MIMO decomposition scheme does not work (e.g., the $4 \times (2,2,2)$ configuration).

A close observation of the performance in the configuration $5 \times (3,3)$ shows that the performance of the proposed scheme is much better than that of the standard MU-MIMO

decomposition scheme. This is because the standard MU-MIMO decomposition scheme becomes inefficient with respect to transmit power as discussed in Section II when the number of transmit antennas is not large enough. When there are enough transmit antennas (e.g., $M = 6$ in Figure 4), it can be observed that the standard MU-MIMO decomposition scheme performs close to the proposed scheme. Therefore, it is good to use the standard MU-MIMO decomposition in such a case because it has lower complexity.

When the channel is correlated, the standard MU-MIMO decomposition scheme also becomes inefficient with respect to transmit power as discussed in Section II. This can be observed in Figure 5, where a $6 \times (2,2)$ system in a highly spatially correlated channel with one departure wave with 5° of angle spread is investigated. We can see that the proposed scheme always outperforms the standard MU-MIMO decomposition scheme. This is because the null space $\text{null}(\mathbf{H}_k)$ may have large overlap with the joint null-space $\bigcap_{i=1, i \neq k}^K (\mathbf{H}_i)$ and this reduces the efficiency of the standard decomposition scheme in terms of transmit power. The phenomenon of the small capacity at low outage probability in those schemes that separate users by space, is caused by the similar null spaces $\text{null}(\mathbf{H}_k)$ and $\bigcap_{i=1, i \neq k}^K (\mathbf{H}_i)$. When the null space $\text{null}(\mathbf{H}_k)$ is similar to the joint null space $\bigcap_{i=1, i \neq k}^K (\mathbf{H}_i)$ or $\text{null}(\mathbf{H}_k) \equiv \bigcap_{i=1, i \neq k}^K (\mathbf{H}_i)$, users are difficult to be separated by

space. In reality, one has to avoid such situation by using user clustering that clusters those users that can be well separated by space to transmit simultaneously.

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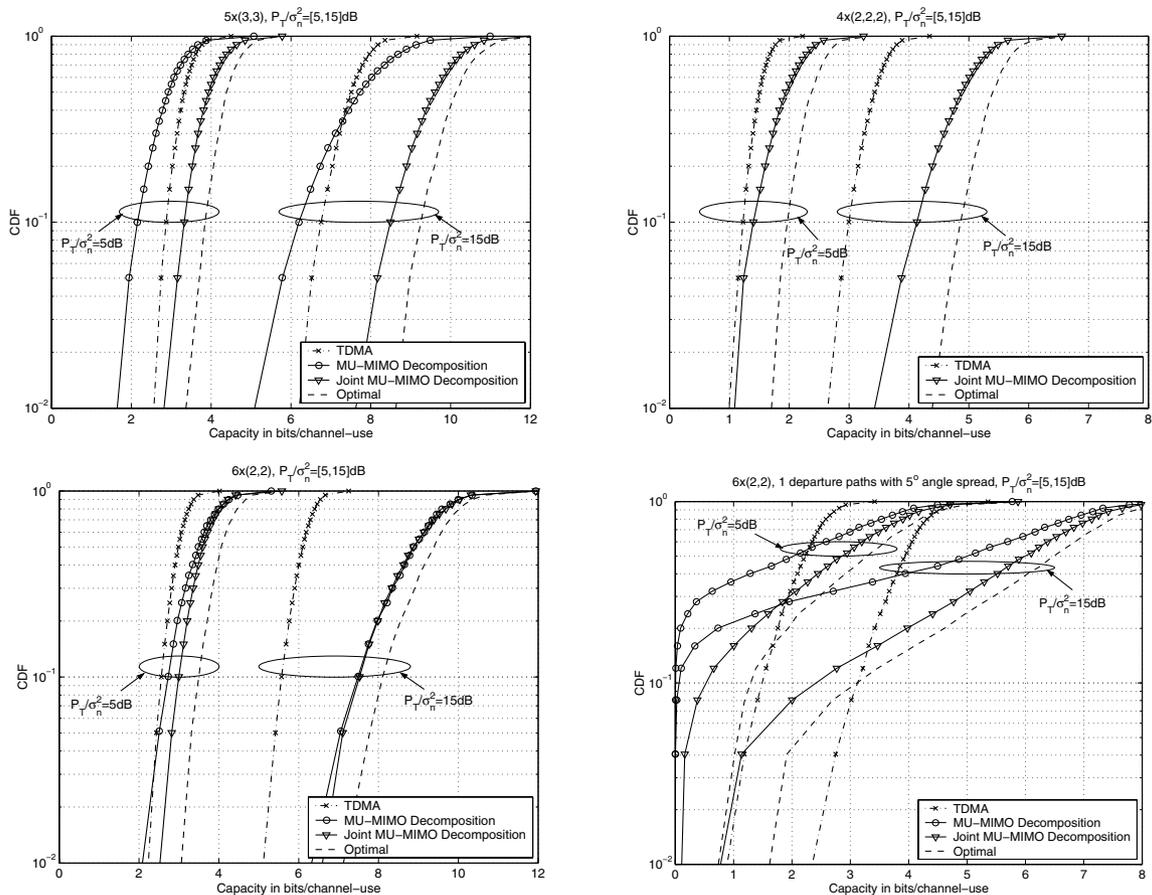


Figure 2 to Figure 5: Upper Left - Figure 2; Upper Right - Figure 3; Lower Left - Figure 4; Lower Right - Figure 5